UNITED STATES PATENT APPLICATION

for

AN LPC FILTER FOR REMOVING PERIODIC AND QUASI-PERIODIC INTERFERENCE FROM SPREAD SPECTRUM SIGNALS

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AN LPC FILTER FOR REMOVING PERIODIC AND QUASI-PERIODIC INTERFERENCE FROM SPREAD SPECTRUM SIGNALS

FIELD OF THE INVENTION

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The present invention relates to using a linear predictive coding filter for the purpose of removing periodic and/or quasi-periodic interference from spread spectrum signals.

10   ## BACKGROUND OF THE INVENTION

Wireless communications has emerged to become a huge market as millions of people world-wide buy cellular handsets, subscribe to Personal Communications Services (PCS), and make calls on a daily basis. There are

15   many competing technologies in the wireless communications field. Initially, cellular transmissions were made according to traditional analog radio frequency (RF) technology. But as wireless digital technology improved, it became clear that digital applications were far superior to that of analog. The three dominant wireless digital technologies existing today include Global

20   System of Mobile communications (GSM), Time Division Multiple Access (TDMA), and Code Division Multiple Access (CDMA). Of these three digital wireless technologies, CDMA is gaining widespread popularity because of its many advantages.

Generally, CDMA offers greater signal quality, resulting in clearer calls. In addition, CDMA utilizes a spread-spectrum approach, which essentially entails spreading the signal out across a wider spectrum. Consequently, the overall power of the transmitted signal can be boosted

5   without exceeding the FCC regulations in any one channel. This makes it ideal for deployment in dense urban areas where multi-pathing is an issue. In turn, this results in fewer dropped calls. Furthermore, CDMA technology is more power efficient, thereby prolonging the standby and active battery life. But one of the most attractive features of CDMA is that it offers a greater

10 capacity for carrying signals. Basically, the airwaves are divided into a number of different frequency bands per Federal Communications Commission (FCC) regulations. A limited segment of the airwaves has been allocated by the FCC for cellular usage. Due to the huge demand for cellular usage and the limited bandwidth that is available, getting a license from the

15 FCC to transmit on a particular frequency band is extremely expensive. By increasing capacity, CDMA enables PCS providers to carry more users per channel. This increased capacity directly translates into greater revenue for cellular companies.

20 The advantages of CDMA carry over into high-speed wireless digital access. Increasingly, wireless digital applications are being used to access digital data (e.g., the Internet, intranet, multimedia, business data, etc.) at high speeds. With high speed wireless access, mobile users can obtain instant access to the Internet, business data (e.g., stock market quotes, sales reports,

25 inventory information, price checks, customer data, emails, pages, etc.), and

other real time data (e.g., traffic updates, weather information, sports news, etc.). The goal is to provide cellular handsets, personal digital assistants, portable communications devices, etc. the ability to transmit and receive digital data as well as make conventional telephone calls. The trend is

5   towards ever faster mobile data speeds to meet customer demands. With greater data speeds, it is possible to provide even more data to more users. Recent CDMA based standards such as IS-95 and 3G are proposing increased data rates and capabilities. Other emerging standards include IEEE 802.11(b) which utilizes a direct sequence spread spectrum technique and "Bluetooth"

10 which utilizes a frequency hopping spread spectrum technique.

Unfortunately, spreading the signal out across a wide spectrum subjects that signal to a greater degree of interfering signals found within that spectrum. Whereas digital filters can be used to effectively notch out all the

15 known, fixed interference being broadcast in designated restricted bands, it is virtually impossible to accurately quantify and then effectively notch out each of the huge host of variable interfering signals in the various non-restricted bands. The aggregate effect from all of the various interference sources dramatically reduces the range of a spread spectrum signal. Furthermore, the

20 interference significantly reduces the rate by which data can be transmitted using a spread spectrum technique.

Thus, there is a need in the prior art for a method or apparatus which could somehow eliminate most if not all of the interference so as to effectively

increase the range and rate by which spread spectrum signals may be transmitted and received.

SUMMARY OF THE INVENTION

The present invention pertains to an apparatus and method for using a linear predictive coding filter for the purpose of removing periodic and/or

5   quasi-periodic interference from spread spectrum signals. Data is encoded and transmitted as a spread spectrum signal. Periodic and quasi-periodic signals which act as interference in the spectrum of interest is effectively filtered out by using a linear predictive coding filter. The LPC filter takes a digitized received spread spectrum signal and generates a set of predictive

10   coefficients and a set of error coefficients. The predictive coefficients represent the interfering periodic and/or quasi-periodic signals. As such, this set of predictive coefficients are discarded. The remaining error coefficients represent what is left over and thereby contains the useful transmitted data found within the spread spectrum signal. The error coefficients are used by

15   the signal processing block to extract the transmitted data. By implementing the LPC filter in such a novel and unique way, the present invention dramatically improves the range and data rate by which spread spectrum systems may operate.

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BRIEF DESCRIPTION OF THE DRAWINGS

The present invention is illustrated by way of example, and not by way of limitation, in the figures of the accompanying drawings and in which like

5   reference numerals refer to similar elements and in which:

Figure 1 shows an exemplary baseband direct sequence, spread spectrum CDMA receiver upon which the present invention may be practiced.

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Figure 2 shows an exemplary circuit diagram of a linear predictive coding (LPC) filter having a gradient adaptive lattice structure.

Figure 3 shows how the difference signal e(n) or prediction error is

15   calculated.

Figure 4 shows a feedback loop with with a FIR filter.

Figure 5 is a block diagram showing how the LPC filter is used in the

20   present invention.

Figure 6 is a flowchart describing the steps of implementing an LPC filter to filter out periodic and/or quasi-periodic signals in a spread spectrum signal.

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DETAILED DESCRIPTION

An apparatus and method for using a linear predictive coding filter for the purpose of removing periodic and/or quasi-periodic interference from

5   spread spectrum signals is disclosed. In the following description, for purposes of explanation, numerous specific details are set forth in order to provide a thorough understanding of the present invention. It will be obvious, however, to one skilled in the art that the present invention may be practiced without these specific details. In other instances, well-known

10   structures and devices are shown in block diagram form in order to avoid obscuring the present invention.

Figure 1 shows an exemplary baseband direct sequence, spread spectrum CDMA receiver upon which the present invention may be

15   practiced. The CDMA receiver uses Walsh functions and a separate pseudo-random code . The RF signal is received over antenna 101. The signal is then amplified by an amplifier 102. In the currently preferred embodiment, amplifier 102 is comprised of two or more baseband video amplifiers coupled in series. This can provide a gainbandwidth product in the Terahertz range.

20   Next, the analog signal is converted into an equivalent digital signal by an analog-to-digital converter 103. A linear predictive coding filter 104 is then used to filter out the periodic and quasi-periodic interference in the spectrum of interest. Thereupon, the signal is demodulated by multiplying it with the synchronized pseudo-random number 105. This is the same pseudo-random

25   number associated with the transmitting base station. The signal is

multiplied by a synchronized Walsh function 106 in order to eliminate interference due to other users' transmission within that cell. An integration 107 is followed by a sample and hold 108 function. Optionally, a bandpass filter is used to filter out the AM radio signals (e.g., 0.5 MHz to 1.5 MHz).

5   Furthermore, a high pass filter may used to filter out the higher frequencies (e.g., above 30 MHz). Alternatively, notch filter(s) may be used to filter out the known interference signal(s) in the restricted bands.

It should be noted that the present invention works with any type of

10 spread spectrum technique and at any frequency. The present invention can be implemented for cell phone, data transfers, peer-to-peer communications, satellite, military, commercial, civilian, IEEE 802.11(b), Bluetooth, as well as a wide range of different wireless transmissions schemes, formats, and medium. One such spread spectrum system is described in detail in the

15 patent application entitled, "A Baseband Direct Sequence Spread Spectrum Transceiver," filed January 26, 2001, Serial No. 09/772,110 and which is incorporated by reference in its entirety herein. Another spread spectrum system is described in the patent application entitled, "Application of a Pseudo-Randomly Shuffled Hadamard Function In A Wireless CDMA

20 System," filed December 5, 2000, Serial No. 09/730,697 and which is incorporated by reference in its entirety herein.

In the currently preferred embodiment of the present invention, a linear predictive coding (LPC) filter is used to filter out periodic and quasi-

25 periodic signals in the band of interest. LPC type filters are well known in the

art. (See, for example, L. R. Rabiner and R. W. Schafer, *Digital Processing of Speech Signals*; N. Morgan and B. Gold, *Speech and Audio Signal Processing : Processing and Perception of Speech and Music*; J. R. Deller, J. G. Proakis, and J. H. L. Hansen, *Discrete-Time Processing of Speech Signals*; S. Furui, *Digital Speech*

5   *Processing, Synthesis and Recognition*; D. O'Shaughnessy, *Speech Communications : Human and Machine*; A. J. Rubio Ayuso and J. M. Lopez Soler, *Speech Recognition and Coding : New Advances and Trends*; M. R. Schroeder, *Computer Speech: Recognition, Compression, Synthesis*; B. S. Atal, V. Cuperman, and A. Gersho, *Speech and Audio Coding for Wireless and Network*

10   *Applications*; B. S. Atal, V. Cuperman, and A. Gersho, *Advances in Speech Coding*; D. G. Childers, *Speech Processing and Synthesis Toolboxe*; R. Goldberg and L. Rick, *A Practical Handbook of Speech Coders*.)

They are found in many audio applications for the coding of audio

15   and/or speech signals. In the prior art, the purpose for LPC filters is to determine linear predictive terms which are critical in modeling speech. Figure 2 shows an exemplary circuit diagram of a linear predictive coding (LPC) filter having a gradient adaptive lattice structure. The LPC filter of Figure 2 is described in detail in the publication by Florian Keiler, Daniel

20   Arfib, and Udo Zolzer, "Efficient Linear Prediction For Digital Audio Effects," Proceedings of the COST G-6 Conference on Digital Audio Effects (DAFX-00), Verona, Italy, December 7-9, 2000.

According to the publication, in LPC, the current input sample x(n) is approximated by a linear combination of past samples of the input signal. The prediction of x(n) is computed using an FIR filter by

$$\hat{x}(n) = \sum_{k=1}^{p} a_k x(n-k)$$

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where p is the prediction order and a k are the prediction coefficients. With the z-transform of the prediction filter

$$P(z) = \sum_{k=1}^{p} a_k z^{-k}$$

10 the difference between the original input signal x(n) and its prediction ^x(n) is evaluated in the z-domain by

$$e(z) = X(z) - \hat{X}(z) = X(z)[1 - P(z)] = X(z)A(z).$$

The difference signal e(n) is called residual or prediction error and its

15 calculation is depicted in Figure 3. Here the feed forward prediction is considered where the prediction is calculated in forward direction from the input signal.

Using the excitation ~e(n) as input to the all-pole filter

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$$H(z) = \frac{1}{1 - P(z)}$$

produces the output signal

25 $$Y(z) = \tilde{E}(z) \cdot H(z)$$

where H(z) can be realized with the FIR filter P (z) in a feedback loop as shown in Figure 4. If the residual e(n) calculated in the analysis stage is fed directly into the synthesis filter, the input signal x(n) will be ideally

5   recovered.

The IIR filter H(z) is termed synthesis filter or LPC filter and it models - except for a gain factor - the input signal X(z). For speech coding this filter models the time-varying vocal tract. The filter A(z) = 1 - H(z) for calculating

10   the residual from the input signal is called the inverse filter.

With optimal filter coefficients, the residual energy is minimized. This can be exploited for efficient coding of the input signal where the quantized residual ~e(n) = Q{e(n)} is used as excitation to the LPC filter. Three

15   commonly used linear prediction methods (autocorrelation method, Burg algorithm, and gradient adaptive lattice) are presented to get methods which are suited for real-time computation, i.e. to get a similar workload each sample. We consider here linear prediction methods for a computation of the residual with zero delay. Thus, the prediction coefficients are computed from

20   past samples of the input signal and the methods are suited for audio coding using the ADPCM structure where no transmission of the filter coefficients is required. The fast filter update coming from the similar workload each sample leads to better spectral models than block-based approaches where the coefficients are held constant for the duration of one block. With a fast

update of the spectral model no interpolation of the filter coefficients between frames is required.

The prediction error can be calculated by a standard FIR structure which requires the direct FIR coefficients a_k. In the lattice structure of Figure 2, the signals $f_m(n)$ and $b_m(n)$ are used which are the forward and backward prediction errors of an m-th order predictor. Forward prediction means the prediction from past samples while in backward prediction, a sample is predicted from future samples. In the lattice methods, the lattice or PARCOR (partial correlation) coefficients k_i are calculated instead of the direct FIR coefficients. Although it is possible to calculate the direct coefficients from the lattice ones, sometimes it is useful to perform the filter operation in the lattice structure. The main advantage of the lattice coefficients is that the stability of the LPC filter is guaranteed for $|k_i| < 1$. Furthermore, if a predictor of order m-1 is already known, for a predictor of order m only the coefficient k_m has to be calculated. For the direct FIR coefficients normally the complete coefficient set has to be changed in this case.

In case of using the lattice structure, the lattice states $b_i(n)$ have to be recalculated if the lattice coefficients k i are changed. This problem does not occur in the direct FIR structure since the filter states are equal to past samples of the input signal and they are independent of the used coefficient set.

Some methods to calculate the prediction coefficients for

minimizing the residual energy is now described. First, the standard block-based approaches of the Burg Algorithm and the autocorrelation method are summarized. Then the sample based gradient adaptive lattice (GAL) method is described. Finally, modifications of the block-based methods for a sample-based calculation in a real-time system is described.

The Burg algorithm is based on the lattice structure and it minimizes for a predictor of order m in a block of length N the sum of the energies of the forward prediction error $f_m(n)$ and of the backward prediction error $b_m(n)$.

The initialization of the forward and backward prediction errors of order zero for the considered block is obtained by

$$f_0(n) = x(n), n = 0, \ldots, N - 1$$
$$b_0(n) = x(n), n = 0, \ldots, N - 1$$

where n denotes the time index in the considered block. For $m = 1, \ldots, p$ the following operations are performed:

Calculation of the m-th lattice coefficient

$$k_m = \frac{2 \sum_{n=m}^{N-1} [f_{m-1}(n) b_{m-1}(n-1)]}{\sum_{n=m}^{N-1} [f_{m-1}^2(n) + b_{m-1}^2(n-1)]}$$

Recursively calculation of the forward and backward pre-diction errors of order m :

$$f_m = f_{m-1}(n) - k_m b_{m-1}(n-1),$$
$$n = m+1,...,N-1$$
$$b_m(n) = b_{m-1}(n-1) - k_m f_{m-1}(n),$$
$$n = m,...,N-1$$

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The autocorrelation method minimizes the prediction error e(n),or in terms of the lattice structure, the forward prediction error. For a block of length N an approximation of the autocorrelation sequence is calculated by

10 $$R(i) = \frac{1}{N} \sum_{n=i}^{N-1} u(n)u(n-i)$$

where u(n) = x(n)* w(n) is a windowed version of the considered block x(n), n = 0, . . . , N - 1. Normally, a Hamming window is used. For a predictor of order p the filter coefficients a i for i = 1, . . . , p are obtained by solving the

15 normal equations

$$\sum_{k=1}^{p} a_k R(i-k) = R(i), i = 1,...,p.$$

An efficient solution of the normal equations is performed by the Levinson-

20 Durbin recursion. First the energy of the predictor of order zero is initialized to $E_0 = R(0)$. Afterwards the following operations are performed for m = 1, . . . , p, where $a_k^{(m)}$ denotes the k-th coefficient of an m-th order predictor.

$$k_m = \frac{R(m) - \sum_{k=1}^{m-1} a_k^{(m-1)} R(m-k)}{E_{m-1}}$$

$$a_m^{(m)} = k_m$$

$$a_k^{(m)} = a_k^{(m-1)} - k_m a_{m-k}^{(m-1)}, k = 1,...,m-1$$

$$E_m = (1 - k_m^2) E_{m-1}$$

As in the block-based Burg algorithm, in the gradient adaptive lattice
method the lattice coefficients are used and the sum of the forward and
backward prediction errors is minimized. Using the approximation of the
error energy of the m-th order predictor

$$\hat{J}_m(n) = f_m^2(n) + b_m^2(n)$$

yields with the steepest decent approach the coefficient update

$$k_m(n+1) = k_m(n) - \mu_m \frac{\partial \hat{J}_m(n)}{\partial k_m(n)}$$

with the gradient weights m. Applying the recursions for the current time
index n leads to

$$\frac{\partial \hat{J}_m(n)}{\partial k_m(n)} = -2[f_m(n)b_{m-1}(n-1) + b_m(n)f_{m-1}(n)]$$

This gives a formula for a sample-by-sample update of the lattice coefficients.

The simplest approach is to choose the μm values constant. Simulations have shown that the optimum value of μ (equal for all orders for simplicity) depends highly on the used signals, the optimum value varies approximately in the range from 1 to 10. Better results are expected for

5　gradient weights which are adaptively dependent on the expectation value of the sum of the forward and backward prediction error energies. An approximation of this expectation value can be recursively calculated by

$$D_m(n) = \lambda D_m(n-1) + [f_{m-1}^2(n) + b_{m-1}^2(n-1)]$$

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where 0<λ<1 influences the weight of older samples. The gradient weights are obtained by

$$2\mu_m = \frac{\alpha}{D_m(n)}$$

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with a constant value α which is normally chosen to α = 1-λ for a recursive formulation of the Burg algorithm.

Both the autocorrelation method and the Burg algorithm require first

20　an initialization process before the prediction coefficients are computed recursively. The real-time computation of a coefficient set of order p is spread over p + 1 samples; one sample for the initialization and one sample each for the p coefficients. Thus, with the counter i = 0, 1, . . . , p, 0, 1, . . . (changing every sample)we get the following procedure:

For i==0 perform the initialization

For i∈ {1,p} calculate the coefficient with index i.

5   In the initialization process (i = 0) the operations are performed for setting
both the forward and backward prediction error of order zero to the input
samples x(n) in the considered block. For i = 1, . . . , p one coefficient k_i is
calculated and applying the recursions of order m = i, the forward and
backward prediction errors of i-th order are computed which are required in

10   the following sample for computing k_{i+1}. The new k_i replaces the previously
used k_i. Since one coefficient is changed, a recalculation of the lattice states
prior to the filter operation is required.

In the Levinson-Durbin recursion the autocorrelation sequence R(i) for

15   i = 0, . . . , p is required. In the initialization process (i = 0) first the input data
block is windowed, where normally a Hamming window is used; then R(0) is
computed. For i ∈ {1; p} the value R(i) is computed followed by the Durbin
recursion of order m = i. Thus, the calculation of the complete set of the
direct FIR coefficients $a_k^{(p)}$ of order p requires p + 1 samples. If the standard

20   FIR structure is used, the use of the coefficients in the filter operation has to
be delayed by p + 1 samples.

Table 2 shows the maximum workloads per sample for calculating the
filter coefficients, i.e. the filter operations to calculate the prediction are not

25   considered. In the GAL the prediction order p has the greatest influence on

the complexity. In this method for each sample p divisions are required which are very expensive on a DSP (but division is no required if μ is fixed). Note that in the Burg algorithm the maximum workload is only influenced by the block length N which is also the case in the autocorrelation method for

5   long blocks.

Method	DSP instructions
suc. Autocorrelation	Max{4N+55,3N+5p+172}
suc. Burg	9N+72
GAL	90p+1

Table 1 Maximum workload per sample for coefficient calculation.

10   In the example given above, it can be seen that the resulting linear predictive terms are given by k_m. In the prior art, the k_m terms are used to model speech. However, note that there are resulting error terms, e(n)=fp(n) and bp(n), which are also generated as an output from the LPC filter. In the prior art, these error terms are simply discarded and not used in any way.

15   However, in the present invention, the error term is kept whereas the linear predictive terms are discarded. In other words, the e(n)=fp(n), bp(n) signals (or any linear combination thereof) are passed on through the receiver, while the k_m signal is discarded.

Figure 5 is a block diagram showing how the LPC filter is used in the present invention. The spread spectrum signal is received by antenna 501. The received signal is then amplified by amplifier or pre-amp 502. The received signal is then digitized by an analog-to-digital (A/D) converter 503.

5 The digital signal is then fed as an input to an LPC filter 504. The error term coming out of the LPC filter 504 is used for further processing by the receiver's signal processor block 505. The linear predictive terms generated by the LPC filter 504 contains the periodic and quasi-periodic signals. These periodic and quasi-periodic signals are actually interference with respect to

10 the spread spectrum signal. As such, these linear predictive terms are intentionally discarded by the present invention, thereby effectively filtering out the interference. Instead, the "error" term, which contains everything except the periodic and quasi-periodic signals, is used by the rest of receiver's signal processing system. Note that the sequence length of the spread

15 spectrum signal should be significantly longer than the order of the lattice. Since the spread spectrum signal is not seen as periodic or quasi-periodic by the lattice, it is unaffected by the lattice; while the periodic and quasi-periodic interference is removed. Thereby, the present invention entails using an LPC filter in a novel and hitherto unconventional way to effectively remove

20 everything in the band of interest which is periodic or quasi-periodic in nature.

Figure 6 is a flowchart describing the steps of implementing an LPC filter to filter out periodic and/or quasi-periodic signals in a spread spectrum signal. Initially, a spread spectrum signal is received, step 601. This received

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spread spectrum signal is then digitized, step 602. In step 603, a gradient

adaptive lattice LPC filter takes this digitized spread spectrum signal and

generates a set of prediction coefficients and a set of error coefficients. The set

of prediction coefficients corresponds to periodic and quasi-periodic (if any)

5   signals found in the received spread spectrum signal. These periodic and

quasi-periodic signals represent "interference" with respect to the data

contained within the spread spectrum system. As such, the prediction

coefficients are discarded. The information left over is represented in the

error coefficients. This contains the useful data contained in the spread

10   spectrum signal which was transmitted by a corresponding spread spectrum

transmitter. Consequently, the error coefficients are used by the signal

processor to recover the useful data, step 605.

It should be noted that the present invention can be applied to any

15   modulation scheme, either wireless or hard-wired, which utilizes a spread-

spectrum technique. In particular, the present invention can be applied to

CDMA cellular handsets as well as other wireless mobile CDMA devices or

appliances. Furthermore, the present invention can be expeditiously applied

to peer-to-peer wireless applications, especially for peer-to-peer cellular

20   voice and/or data communications. The present invention can be applied to

increase the range and/or data rates of existing spread spectrum techniques,

including but not limited to CDMA, IEEE 802.11(b), Bluetooth, 3G, etc. One

such system upon which the present invention may be practiced is described

in the patent application entitled, "A Communications Network Quality Of

25   Service System And Method For Real Time Information," filed December 12,

2000, Serial Number 09/738,010, which is incorporated by reference in its

entirety herein. In addition, the present invention works with any type of

filter which has the property of discriminating periodic and/or quasi-periodic

signals, including but not limited to LPC filters, adaptive gradient lattice

5   filters, etc.

Therefore, a linear predictive coding filter for the purpose of removing

periodic and/or quasi-periodic interference from spread spectrum signals is

disclosed. The foregoing descriptions of specific embodiments of the present

10   invention have been presented for purposes of illustration and description.

They are not intended to be exhaustive or to limit the invention to the precise

forms disclosed, and obviously many modifications and variations are

possible in light of the above teaching. The embodiments were chosen and

described in order to best explain the principles of the invention and its

15   practical application, to thereby enable others skilled in the art to best utilize

the invention and various embodiments with various modifications as are

suited to the particular use contemplated. It is intended that the scope of the

invention be defined by the Claims appended hereto and their equivalents.

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